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### (54) Low power pre-regulator power supply circuit

Niederleistung-Vorreglerstromversorgungsschaltung

Circuit d'alimentation prérégulateur à basse puissance

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**EP-A- 0 256 569 DE-A- 3 304 759  
GB-A- 2 208 019**

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## Description

This invention relates to power supply circuits, and particularly, to a low power transformerless, inductorless power supply circuit of the switching type, and more particularly to a switching type regulated power supply for energizing a load comprising:

first and second input terminals for supplying a pulsatory type rectified voltage to the power supply, a load capacitor and a switching transistor in a series circuit connected across the first and second input terminals,  
 a pair of output terminals coupled to the load capacitor, and  
 a control circuit having input means coupled to the switching transistor and an output coupled to a control electrode of the switching transistor.

Such a switching type regulated power supply is known from European Patent Application EP-A-0 256 569.

One common form of power supply, which can be found in certain TV receivers, consists of a full wave bridge rectifier, a load capacitor (e.g. 330 $\mu$ F), and a linear regulator. The bridge rectifier generates a voltage which is filtered by the load capacitor. The load capacitor voltage is then fed to the linear regulator which in turn regulates the voltage at a preselected level, for example, 130V.

This power supply has certain disadvantages and limitations. For a 120V AC input, 170V is generated across the load capacitor of the bridge rectifier. Since the linear regulator must produce an output voltage of 130V, there is a 40V drop across the regulator itself, drawing up to 1 amp of current. In order to protect the regulator from damage due to the excessive amount of dissipated power, a number of thermal resistors are connected in parallel with the regulator so as to shunt a part of the current. These resistors are bulky and thus are undesirable as they increase the cost of the overall system and furthermore occupy a significant amount of space on the TV board. In addition, they allow only a small variation in the line voltage because if the voltage rating of the load capacitor is exceeded, damage to the load capacitor as well as the linear regulator may occur. This power supply therefore requires a well regulated 120V commercial line voltage. Since the load capacitor is charged only once for each half cycle of the AC supply voltage, higher peak capacitor charge currents result, along with other attendant difficulties.

U.S. Patent 4,685,046 (8/4/87) describes a transformerless, low voltage, direct current power supply of the switching type adapted to energize a low voltage direct current load. A full-wave bridge rectifier is coupled directly across a 115V, 60Hz alternating current line to provide a 120Hz pulsating direct current. A pair of transistors, alternately switching on and off in complemen-

tary fashion, continuously applies to a low power load only a leading edge portion and a trailing edge portion of each of the 120Hz direct current pulses. The resultant direct current voltage, e.g. 11.3 peak volts across the

5 load, is thus substantially reduced to a desirable level as compared ( to the peak voltage (161 peak volts) of the pulsating direct current provided at the bridge output. In another embodiment, the function of the transistors is provided by a pair of operational amplifiers which 10 control the switching of a field effect transistor in series with the load. The control function is provided by sensing the input voltage of the power supply circuit. This has the disadvantage that if the input changes too abruptly and the sensor is not able to respond immediately to the 15 change, the exact value of the output voltage cannot be well controlled. Furthermore, because the circuit threshold level is set by means of a zener diode, this makes the circuit less flexible in the event that the threshold has to be adjusted.

20 Another transformerless power supply which also senses the input supply voltage to determine the output voltage is described in DE 3304759 (8/16/84). In this German patent, a first op-amp compares a first input voltage, supplied by a full wave bridge rectifier, with a

25 DC reference voltage supplied by a zener diode and a resistor voltage divider and a second op-amp compares a second input voltage with the DC reference voltage. If either input voltage is lower than the reference voltage, a switching transistor in series with a load capacitor is 30 turned on. The load capacitor is only charged when the rectified AC supply voltage is below the reference voltage. The control function is once again provided by sensing the input voltage. This circuit uses a highside power switch which produces higher power losses when 35 compared with a low-side switch and results in problems in the integration thereof.

In the switching type regulated power supply disclosed in European Patent Application EP-A-0 256 569 the control circuit operates only in dependence of the 40 drain-source voltage of the switching transistor.

UK Patent Application GB-A-2 208 019 shows a switching type regulated power supply having a control circuit which controls the switching transistor in dependence of the voltage across the load capacitance.

## SUMMARY OF THE INVENTION

An object of the present invention is to provide an 50 integrated circuit low cost power supply that produces a regulated DC voltage across a load capacitor from a wide input voltage range, in particular, one which can be used with both 120V and 220V AC line voltages.

Another object of the invention is to provide a power 55 supply pre-regulator circuit that overcomes the disadvantages and limitations of known circuits of this type. In particular, one that senses the output voltage instead of the input voltage.

A further object of the invention is to provide a power

supply pre-regulator circuit with reduced charging currents of the load capacitor while keeping the power dissipation to a minimum.

A still further object of the invention is to provide a power supply in which the switching losses in the switching transistor are kept low by monitoring the power switching transistor so that it is switched only when its drain-source voltage ( $V_{ds}$ ) is below a safe level, for example, 60V.

Another object of the invention is to provide a power supply system which eliminates the need for bulky thermal shunt resistors and hence reduces the thermal dissipation of the system.

These and other objects and advantages are achieved by means of the switching type regulated power supply as defined in the opening paragraph which is characterized in that said control circuit includes means responsive to a differential voltage of the load capacitor for turning off the switching transistor at a first predetermined voltage level of the output load capacitor voltage and means responsive to a voltage produced across the switching transistor for turning on the switching transistor at a second predetermined voltage level of the switching transistor.

The novel integrated circuit power supply system charges the load capacitor during the rising edge of the input cycle.

The system includes a control circuit that senses the output voltage across the load capacitor and whenever the capacitor voltage exceeds a preset voltage level, for example, 150V, it turns off a series connected switching transistor, such as a field effect transistor (FET), which stops the load capacitor from being charged. The full-wave rectified AC sinusoidal supply voltage is applied to the series circuit of the load capacitor and the switching transistor and, during the falling edge of the rectified half cycle of the supply voltage, the control circuit senses when the drain-source voltage of the switching transistor reaches a preset safe level (e.g. 60V) and in response switches on the power switching transistor to charge the load capacitor for a second time during that cycle until the input voltage drops below the capacitor voltage. The transistor switch remains on so that on the next leading (rising) edge of the rectified supply voltage, i.e. when the supply voltage again exceeds the load capacitor voltage, the load capacitor is once again recharged. The control circuit then switches off the series connected switching transistor when the load capacitor voltage (i.e., the output voltage) again exceeds the preset voltage level (e.g. 150V). In this way, the load capacitor is charged twice during each half cycle of the AC supply voltage (or twice during each cycle of the rectified pulsatory voltage at the output of the full wave bridge rectifier circuit).

The load voltage can thus be regulated to any preset threshold level that is determined by a reference voltage. Unlike previous methods, this level would not be affected by the amplitude or rate of change of the input

voltage. The switching transistor is a low-side switch in common source configuration which has the advantages of low power loss and ease of implementation and integration. The dual charging technique of the load capacitor minimizes the ripple voltage across the load.

5 An advantage of this so-called output sensing approach in which the load capacitor voltage and the switching transistor drain-source voltage are monitored rather than the input voltage is that it maintains direct 10 control of the load capacitor voltage while charging the capacitor twice in each cycle. This has a very real advantage in that the output voltage can be more accurately regulated over a much wider range of input voltage.

15 To summarize, the control circuit senses the load capacitor voltage and when it exceeds the preset level (e.g. 150V), the switching transistor is turned off. The control circuit also senses the drain-source voltage and allows the switching transistor to be turned back on 20 when its drain-source voltage falls below a safe level (e.g. 60V). This allows the load capacitor to be charged a second time to produce a second peak. The switching losses are kept to a minimum by switching the switching transistor only when its drain-source voltage is below the 25 safe level. The peak charging currents of the load capacitor are maintained at a low value and the circuit power dissipation is kept at a minimum.

#### BRIEF DESCRIPTION OF THE DRAWINGS

30 A fuller understanding of the invention together with other features, objects and advantages thereof will become apparent from the following detailed description taken in conjunction with the accompanying drawings, 35 in which:

40 Fig. 1 illustrates a simplified block diagram of a preferred embodiment of a power supply in accordance with the present invention,  
Fig. 2 provides waveform diagrams illustrating the operation of the circuit of Fig. 1, and  
Fig. 3 is a more complete schematic circuit diagram showing one way in which the invention shown in Fig. 1 can be realized.

#### DESCRIPTION OF THE PREFERRED EMBODIMENTS

50 Fig. 1 shows a block diagram of a pre-regulator power supply employing the capacitor dual charging concept of the present invention. A conventional, commercial power source 10 of 115V or 220V sinusoidal alternating current at a frequency of 60Hz or the like is coupled to a pair of input terminals of a full-wave bridge rectifier 11 made up of four diodes. The output of the bridge will provide a pulsating rectified voltage,  $V_{in}$ , between a positive voltage line 12 and a negative voltage line 13.

An electric load 14 is connected in parallel with a filter or load capacitor 15 and this parallel combination is connected in series circuit with a switching transistor 16 of a power FET type that can handle the load current. The switching transistor 16 is preferably connected to the low voltage side of the DC supply voltage which thus simplifies its integration into an integrated circuit. The field effect transistor is preferably chosen to be an LIG-BT power device or an LDMOS device. Of course, the invention is not limited to this choice of the power devices.

A control circuit 21 includes a subtractor circuit 17 which is coupled across the terminals of the load capacitor 15 in order to sense the capacitor voltage. A means for differential voltage sensing is required rather than a single-ended voltage sensor. The subtractor circuit 17 may or may not include a hysteresis circuit, which helps suppress any spurious inputs caused by ringing produced during turnoff of the switching transistor 16.

The output of the subtractor circuit 17 is connected to the non-inverting input (+) of a comparator 18. The inverting input (-) of the comparator 18 is connected to a terminal 19 which supplies a preset reference voltage,  $V_{ref}$ . The reference voltage  $V_{ref}$  determines the voltage level at which the comparator 18 will change state and can be adjustable, if desired. In one example, useful in a TV receiver, the reference voltage  $V_{ref}$  was selected so that the comparator 18 changes state when the load capacitor voltage  $V_{cap}$  across the load capacitor 15 exceeds 150V.

A sensor circuit 20 is provided in order to sense the drain-source voltage  $V_{ds}$  of the switching transistor 16. As will be shown below, the  $V_{ds}$  sensor circuit 20 may comprise a second comparator circuit which compares the voltage  $V_{ds}$  of the switching transistor 16 to a reference voltage which, in the present example, is chosen so that the second comparator will change state when the drain-source voltage of the power switching transistor drops below 60V.

An output of the comparator circuit 18 and of the  $V_{ds}$  sensor circuit 20 are each connected to a respective input of a logic circuit 22, which in its simplest form could consist of a NOR gate.

The output of the logic circuit 22 is in turn coupled to an input of a driver amplifier 23. The output of the driver amplifier is coupled to the gate electrode of the power switching transistor 16.

A pair of DC output terminals coupled to the load capacitor 15 can supply the load capacitor voltage to a linear regulator circuit or the like (not shown).

The operation of the circuit of Fig. 1 will be described in connection with the voltage waveform diagram shown in Fig. 2. The bridge rectifier 11 circuit supplies a rectified pulsating voltage waveform  $V_{in}$  as shown in Fig. 2. In the case of a 60Hz AC supply voltage, the voltage  $V_{in}$  has frequency of 120Hz. The voltage  $V_{in}$  is applied across the series circuit consisting of the load capacitor 15 and the switching transistor 16.

The function of the control circuit 21 is to regulate the voltage  $V_{cap}$  across the load capacitor 15 to a preset voltage level, for example, 150V DC, despite the fact that the input voltage  $V_{in}$  has a peak value that is higher than the preset voltage. Initially, assuming the load capacitor 15 is uncharged, the switching transistor 16 is turned on fully so that substantially the entire voltage  $V_{in}$  is across the load capacitor 15. This will allow the load capacitor 15 to be charged as the voltage  $V_{in}$  rises, i.e. as  $V_{in}$  rises in voltage, the capacitor voltage  $V_{cap}$  also increases.

The subtractor circuit 17 continuously monitors the differential voltage  $V_{cap}$  and by means of the comparator 18 compares  $V_{cap}$  with a preset reference voltage,  $V_{ref}$ , supplied to the inverting input of the comparator 18. When the load capacitor voltage  $V_{cap}$  reaches the preset level, i.e. 150V in the example chosen, the comparator circuit 18 changes state.

The logic circuit 22 responds to the output signal of the comparator circuit 18 to drive the switching transistor 16 into cut-off via a gate turn-off voltage applied to the gate of the switching transistor 16 via the driver amplifier 23. This prevents further charging of the load capacitor 15 as the input voltage  $V_{in}$  increases further in value above the 150V level. This produces a first peak in the capacitor voltage waveform at the instant labelled  $t_1$  on the waveform of Fig. 2. The waveform diagram of Fig. 2 also shows the switch gate voltage waveform  $V_{sw}$ , which goes low at the instant  $t_1$  when the switching transistor is turned off. During the time period after the switch turns off at  $t_1$ , the capacitor discharges slowly through the load resistor 14, as shown by the capacitor waveform  $V_{cap}$  in Fig. 2.

As the voltage  $V_{in}$  continues to increase and the load capacitor 15 continues to discharge, the subtractor circuit 17 may include a hysteresis circuit to maintain the comparator circuit 18 in the state to hold the switching transistor 16 off via the logic and driver stages 22 and 23. The hysteresis circuit can be implemented by changing the value of the reference voltage  $V_{ref}$  when the comparator 18 switches states. During the time period when the switching transistor 16 is turned off, the drain-source voltage of switching transistor 16 can exceed 60V.

After the voltage  $V_{in}$  reaches its peak value and begins its descent, the drain-source voltage,  $V_{ds}$ , of the switching transistor 16 will begin to decrease. The voltage  $V_{ds}$  satisfies the relation,

$$V_{ds} = V_{in} - V_{cap}.$$

When the voltage  $V_{ds}$  drops below a second preset level, in the present example, 60V, the  $V_{ds}$  sensor circuit 20 will be triggered to change state and in turn cause the logic circuit 22 to turn the switching transistor 16 back on. This will occur at the instant  $t_2$  in the waveform diagram of Fig. 2 and produces a second peak in the load capacitor voltage waveform  $V_{cap}$  as the load ca-

pacitor recharges towards the voltage  $V_{in}$ . The waveform diagram of Fig. 2 also shows the switch voltage waveform  $V_{sw}$  going high at  $t_2$  when the switching transistor 16 is turned on. It is also possible to set the  $V_{ds}$  sensor circuit to a threshold level of zero volts, in which case the circuit will not produce the second voltage peak at time  $t_2$ .

As the voltage,  $V_{in}$ , continues its descent and drops below the capacitor voltage  $V_{cap}$  in the period between  $t_2$  and  $t_3$ , the switching transistor 16 will stay on (be conductive), but will not continue to charge the load capacitor 15 when the voltage  $V_{in}$  has dropped below the value of the capacitor voltage  $V_{cap}$ .

On the rising edge of the next cycle, the voltage,  $V_{in}$ , will increase again until at the instant  $t_3$  when  $V_{in}$  exceeds the capacitor voltage  $V_{cap}$ , the load capacitor 15 will begin to charge again through the still conductive switching transistor 16. The first peak in the capacitor voltage  $V_{cap}$  waveform at a value of 150V will then reappear as the cycle described now repeats itself. The switching transistor 16 will again be turned off when the subtractor circuit senses a differential voltage of 150V across the load capacitor 15.

It can thus be seen that the control circuit 21 allows the load capacitor 15 to be charged twice during each cycle of the rectified voltage waveform  $V_{in}$  (i.e. twice during each half cycle of the AC supply voltage 10). The subtractor circuit 17 initiates the first peak in the capacitor voltage waveform  $V_{cap}$  and the  $V_{ds}$  sensor initiates circuit 20 the second peak. This technique allows the load capacitor 15 to be charged twice in each half cycle of the AC supply voltage thereby lowering the peak charging current flowing to the load capacitor as compared to known methods in which the capacitor is charged only once for each half cycle of the AC supply voltage. The lower peak charging currents resulting from the invention produce lower stresses on the switching transistor 16 and the lower value of  $V_{ds}$  during switching of the switching transistor reduces the switching losses and also the power dissipation. This increases the circuit efficiency and also makes it possible to use a switching transistor that is less expensive since it will be subjected to lower voltages during switching etc.

As can be seen from the foregoing description, the invention can extend the input voltage range of a TV receiver or other electronic apparatus from 120V to 220V or more by limiting the voltage across the load capacitor to a preset level, such as 150V, even if the input voltage reaches a value of 265V, AC (375V peak). The system described insures that the load capacitor voltage does not exceed 150V irrespective of the value of the line voltage. Switching losses are minimal as the switching transistor always switches when the input voltage is about 150V and the drain-source voltage is low. The load capacitor voltage is very well controlled since the capacitor voltage is itself used as the control parameter.

Fig. 3 shows one possible way to realize the complete system of Fig. 1 with the control circuit 21 indicated

by dashed lines. Elements which are the same as those in Fig. 1 have the same reference labels. The subtractor formed by the op-amp 17 attenuates and differentially senses the load capacitor voltage. The subtractor output

5 voltage is then compared to a reference voltage using the comparator 18. The reference voltage has been selected so that the comparator changes state when the load capacitor voltage exceeds 150V. The second comparator 20 is used to sense the drain-source voltage of the FET 16. The input terminals of the second comparator 20 are coupled, either directly or via some means of attenuation, to the drain electrode and the source electrode of the field effect transistor 16. Additional logic 10 uses the signals from the two comparators 18 and 20 to control the turn on and turn off of the power FET 16.

15 In addition to the functional blocks shown in Fig. 1, the control circuit of Fig. 3 also includes a low voltage supply circuit 25 which provides a regulated low DC voltage for energizing the low voltage circuits of the control circuit 21. Fig. 3 also provides a hysteresis circuit 26 which changes the level of the reference voltage supplied to the inverting input of comparator 18 via the reference voltage terminal 19. The duration of the subtractor signal voltage is thereby lengthened by the operation 20 of the hysteresis circuit. The hysteresis circuit is itself conventional. The system of Fig. 3 operates in accordance with the description of the operation of the circuit of Fig. 1 and thus requires no further elaboration.

25 Although a preferred embodiment of the invention 30 has been shown and described, it should be understood that various modifications, deletions and rearrangements of the parts may be resorted to without departing from the scope of the invention as disclosed and claimed herein.

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## Claims

1. A switching type regulated power supply for energizing a load (14) comprising:

40 first (12) and second (13) input terminals for supplying a pulsatory type rectified voltage from an AC voltage source to the power supply, a load capacitor (15) and a switching transistor (16) in a series circuit connected across the first (12) and second (13) input terminals, a pair of output terminals coupled to the load capacitor, and

45 50 55 a control circuit (21) having input means coupled to the switching transistor (16) and an output (23) coupled to a control electrode of the switching transistor (16), characterized in that said control circuit (21) includes means (17) responsive to a differential voltage of the load capacitor (15) for turning off the switching transistor (16) at a first predetermined voltage level of the output load capacitor voltage and means

(20) responsive to a voltage produced across the switching transistor (16) for turning on the switching transistor (16) at a second predetermined voltage level of the switching transistor (16).

2. A switching type regulated power supply as claimed in Claim 1 wherein the control circuit (21) comprises;

a first network (17,18,22) coupled to the load capacitor (15) and responsive to the load capacitor differential voltage for deriving a first switch-type control signal for driving the switching transistor (16) into cut-off at the first predetermined voltage level of the load capacitor voltage, and

a second network (20,21) coupled to the switching transistor (16) and responsive to the transistor voltage for deriving a second switch-type control signal for driving the switching transistor (16) into conduction at the second predetermined voltage level of the switching transistor (16).

3. A switching type regulated power supply as claimed in Claim 2 wherein the control circuit further comprises;

a logic means (22) controlled by said first and second switch-type control signals for supplying a trigger control signal to a control electrode of the switching transistor (16).

4. A switching type regulated power supply as claimed in Claim 1, 2 or 3 wherein said first (12) and second (13) input terminals comprise a high side voltage and a low side voltage, respectively, and said load capacitor (15) and said switching transistor (16) are connected between the first (12) and second (13) input terminals in the order named.

5. A switching type regulated power supply as claimed in Claim 2, 3 or 4 wherein;

said first network comprises a subtractor circuit (15) having its input coupled to the load capacitor (15) and having its output coupled to a first input of a comparator (18), and

wherein a second input of the comparator (18) is coupled to a reference voltage (19) that determines said first predetermined voltage level.

6. A switching type regulated power supply as claimed in Claim 2, 3, 4 or 5 wherein the second network comprises a second comparator (20) having its input coupled across the switching transistor (16).

5 7. A switching type regulated power supply as claimed in Claim 6 wherein the switching transistor (16) comprises a field effect transistor having a drain electrode and a source electrode and the input of the second comparator (20) includes first and second terminals coupled to the drain electrode and the source electrode, respectively, of the field effect transistor.

10 8. A switching type regulated power supply as claimed in Claim 1, 2, 3, 4, 5, 6 or 7 further comprising a full wave bridge rectifier (11) having first and second output terminals coupled to said first (12) and second (13) input terminals, respectively, and a pair of input terminals coupling to a source (10) of sinusoidal AC voltage.

15 9. A switching type regulated power supply as claimed in Claim 8 wherein said bridge rectifier (11) supplies a rectified sine wave voltage to said first (12) and second (13) input terminals and said control circuit (21) is operative to turn off the switching transistor (16) at a given voltage level on the leading edge of the rectified sine wave voltage and to turn on the switching transistor (16) during the trailing edge of the sine wave voltage and at a preset voltage developed across the switching transistor (16).

20 10. A switching type regulated power supply as claimed in Claim 1, 2, 3, 4, 5, 6, 7, 8 or 9 wherein the first predetermined voltage level is less than the peak input voltage value of the pulsatory type rectified voltage.

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## Patentansprüche

1. Schaltende geregelte Stromversorgungsschaltung zum Speisen einer Last (14) mit:

einer ersten (12) und zweiten (13) Klemme zum Liefern einer pulsförmigen gleichgerichteten Spannung von einer AC-Spannungsquelle zu der Stromversorgung,

einem Lastkondensator (15) und einem Schalttransistor (16), die über die erste (12) und die zweite (13) Eingangsklemme in Reihe geschaltet sind,

einem Paar mit dem Lastkondensator gekoppelter Ausgangsklemmen, und

einer Steuerschaltung (21) mit Eingangsmitteln, die mit dem Schalttransistor (16) gekoppelt sind und mit einem Ausgang (23), der mit einer Steuerelektrode des Schalttransistors (16) gekoppelt ist, dadurch gekennzeichnet, daß die genannte Steuerschaltung (21) Mittel (17) aufweist, die eine differenzielle Spannung des Lastkondensators (15) liefern zum Ab-

schalten des Schalttransistors (16) bei einem vorbestimmten Spannungspegel der Ausgangs-Lastkondensatorspannung und Mittel (20) zum Liefern einer an dem Schalttransistor (16) erzeugten Spannung zum Einschalten des Schalttransistors (16) bei einem zweiten vorbestimmten Spannungspegel des Schalttransistors (16).

2. Schaltende geregelte Stromversorgungsschaltung nach Anspruch 1, wobei die Steuerschaltung (21) die nachfolgenden Elemente aufweist:

ein ersten mit dem Lastkondensator (15) gekoppeltes Netzwerk (17, 18, 22), das verantwortlich ist für die differenzielle Lastkondensatorspannung zum Ableiten eines ersten schaltenden Steuersignals zum Betreiben des schaltenden Transistors (14) in den gespererten Zustand bei dem ersten vorbestimmten Spannungspegel der Lastkondensatorspannung, und  
ein zweites mit dem schaltenden Transistor (16) gekoppeltes Netzwerk (20, 21), das verantwortlich ist für die Transistorspannung zum Herleiten eines zweiten schaltenden Steuersignals zum Betreiben des schaltenden Transistors (16) in den leitenden Zustand bei dem zweiten vorbestimmten Spannungspegel des schaltenden Transistors (16).

3. Schaltende geregelte Stromversorgungsschaltung nach Anspruch 2, wobei die Steuerschaltung weiterhin ein logisches Mittel (22) aufweist, das durch das genannte erste und zweite schaltende Steuer- signal gesteuert wird zum Zuführen eines Triggersteuersignals zu einer Steuerelektrode des Schalttransistors (16).

4. Schaltende geregelte Stromversorgungsschaltung nach Anspruch 1, 2 oder 3, wobei die genannte erste (12) und zweite (13) Eingangsklemme eine Hochpegelspannung bzw. eine Tiefpegelspannung aufweist und der genannte Lastkondensator (15) und der genannte Schalttransistor (16) in der genannten Reihenfolge zwischen der ersten (12) und der zweiten (13) Eingangsklemme vorgesehen sind.

5. Schaltende geregelte Stromversorgungsschaltung nach Anspruch 2, 3 oder 4, wobei:

das genannte erste Netzwerk eine Subtrahierschaltung (15) aufweist, deren Eingang mit dem Lastkondensator (15) gekoppelt ist und deren Ausgang mit einem ersten Eingang einer Vergleichsschaltung (18) gekoppelt ist und wobei ein zweiter Eingang der Vergleichsschalt-

tung (18) mit einer Bezugsspannung (19) gekoppelt ist, welche den genannten ersten vorbestimmten Spannungspegel bestimmt.

5 6. Schaltende geregelte Stromversorgungsschaltung nach Anspruch 2, 3, 4 oder 5, wobei das zweite Netzwerk eine zweite Vergleichsschaltung (20) aufweist, deren Eingang über den Schalttransistor (16) gekoppelt ist.

10 7. Schaltende geregelte Stromversorgungsschaltung nach Anspruch 6, wobei der Schalttransistor (16) einen Feldeffekttransistor aufweist mit einer Drain-Elektrode und einer Source-Elektrode und wobei der Eingang der zweiten Vergleichsschaltung (20) eine erste und eine zweite Klemme aufweist, die mit der Drain-Elektrode bzw. der Source-Elektrode des Feldeffekttransistors gekoppelt sind.

15 20 8. Schaltende geregelte Stromversorgungsschaltung nach Anspruch 1, 2, 3, 4, 5, 6 oder 7, weiterhin mit einem Doppelwegbrückengleichrichter (11), dessen erste und zweite Ausgangsklemmen mit den genannten ersten (12) bzw. zweiten (13) Eingangsklemmen gekoppelt sind und mit einem Paar Eingangsklemmen, die zu einer Quelle (10) sinusförmiger AC-Spannung koppeln.

25 30 9. Schaltende geregelte Stromversorgungsschaltung nach Anspruch 8, wobei der genannte Brückengleichrichter (11) der genannten ersten (12) und zweiten (13) Eingangsklemme eine gleichgerichtete sinusförmige Spannung liefert und die genannte Steuerschaltung (21) den Schalttransistor (16) abschaltet bei einem bestimmten Spannungspegel an der Vorderflanke der gleichgerichteten sinusförmigen Spannung und den Schalttransistor (16) während der Rückflanke der sinusförmigen Spannung und bei einer voreingestellten Spannung an dem Schalttransistor (16) einschaltet.

35 40 45 10. Schaltende geregelte Stromversorgungsschaltung nach Anspruch 1, 2, 3, 4, 5, 6, 7, 8 oder 9, wobei der erste vorbestimmte Spannungspegel niedriger ist als der Spitzeneingangsspannungswert der pulsförmigen gleichgerichteten Spannung.

#### Revendications

50 1. Alimentation régulée du type à découpage pour alimenter une charge (14), comprenant :  
55 une première (12) et une deuxième (13) bornes d'entrée pour fournir, à partir d'une source de tension CA, une tension redressée de type pulsatoire à l'alimentation,  
un condensateur de charge (15) et un transistor

de commutation (16) dans un montage en série connecté à la première (12) et la deuxième (13) bornes d'entrée,

une paire de bornes de sortie couplées au condensateur de charge, et un circuit de commande (21) doté de moyens d'entrée couplés au transistor de commutation (16) et une sortie (23) couplée à une électrode de commande du transistor de commutation (16), caractérisé en ce que ledit circuit de commande (21) comprend des moyens (17) réagissant à une tension différentielle du condensateur de charge (15) pour rendre bloquant le transistor de commutation (16) à un premier niveau de tension prédéterminé de la tension de sortie du condensateur de charge et des moyens (20) réagissant à une tension produite dans le transistor de commutation (16) pour rendre passant le transistor de commutation (16) à un deuxième niveau de tension prédéterminé du transistor de commutation (16).

2. Alimentation régulée de type à découpage suivant la revendication 1, dans laquelle le circuit de commande (21) comprend :

un premier réseau (17, 18, 22) couplé au condensateur de charge (15) et réagissant à la tension différentielle du condensateur de charge pour dériver un premier signal de commande de type de commutation pour faire passer le transistor de commutation (16) sur non-conduction au premier niveau de tension prédéfini de la tension du condensateur de charge, et un deuxième réseau (20, 21) couplé au transistor de commutation (16) et réagissant à la tension du transistor pour dériver un deuxième signal de type de commutation pour placer le transistor de commutation (16) en état de conduction au deuxième niveau de tension prédéfini du transistor de commutation (16).

3. Alimentation régulée de type à découpage suivant la revendication 2, dans laquelle le circuit de commande comprend en outre :

des moyens logiques (22) commandés par lesdits premier et deuxième signaux de commande de type de commutation pour fournir un signal de commande de déclenchement à une électrode de commande du transistor de commutation (16).

4. Alimentation régulée de type à découpage suivant la revendication 1, 2 ou 3, dans laquelle lesdites première (12) et deuxième (13) bornes d'entrée comprennent respectivement une tension de haut potentiel et une tension de bas potentiel et ledit con-

densateur de charge (15) et ledit transistor de commutation (16) sont connectés entre la première (12) et la deuxième (13) bornes d'entrée, dans cet ordre.

5. Alimentation régulée de type à découpage suivant la revendication 2, 3 ou 4, dans laquelle :

ledit premier réseau comprend un circuit de soustraction (15) dont l'entrée est couplée au condensateur de charge (15) et dont la sortie est couplée à une première sortie d'un comparateur (18), et dans laquelle une deuxième entrée du comparateur (18) est couplée à une tension de référence (19) qui détermine ledit premier niveau de tension prédéfini.

6. Alimentation régulée de type à découpage suivant la revendication 2, 3, 4 ou 5, dans laquelle le deuxième réseau comprend un deuxième comparateur (20) dont l'entrée est couplée aux bornes du transistor de commutation (16).

7. Alimentation régulée de type à découpage suivant la revendication 6, dans laquelle le transistor de commutation (16) comprend un transistor à effet de champ muni d'une électrode de drain et d'une électrode de source et l'entrée du deuxième comparateur (20) comprend une première et une deuxième bornes couplées respectivement à l'électrode de drain et à l'électrode de source du transistor à effet de champ.

8. Alimentation régulée de type à découpage suivant la revendication 1, 2, 3, 4, 5, 6 ou 7 comprenant de plus un redresseur à deux alternances en pont (11) doté d'une première et d'une deuxième bornes de sortie couplées respectivement aux première (12) et deuxième (13) bornes d'entrée, et une paire de bornes d'entrée couplées à une source (10) de tension CA sinusoïdale.

9. Alimentation régulée de type à découpage suivant la revendication 8, dans laquelle ledit redresseur en pont (11) fournit une tension sinusoïdale redressée auxdites première (12) et deuxième (13) bornes d'entrée et ledit circuit de commande (21) est à même de rendre le transistor de commutation (16) non conducteur à un niveau de tension donné sur le front avant de la tension sinusoïdale redressée et de rendre le transistor de commutation (16) conducteur pendant le front arrière de la tension sinusoïdale et à une tension prédéfinie développée dans le transistor de commutation (16).

10. Alimentation régulée de type à découpage suivant la revendication 1, 2, 3, 4, 5, 6, 7, 8 ou 9, dans laquelle le premier niveau de tension prédéfini est inférieur à la valeur de tension d'entrée de crête de

la tension redressée de type pulsatoire.

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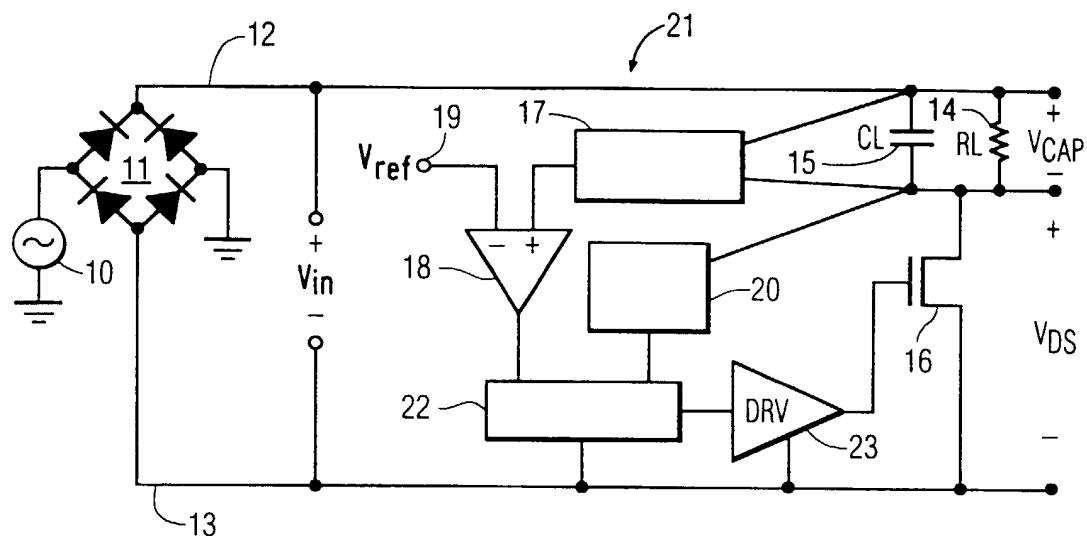


FIG. 1

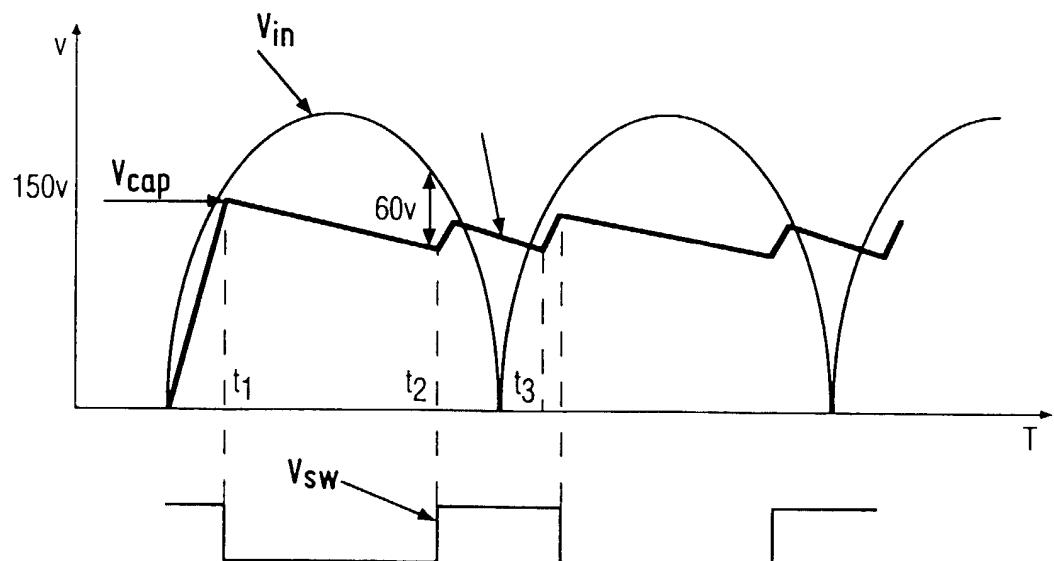
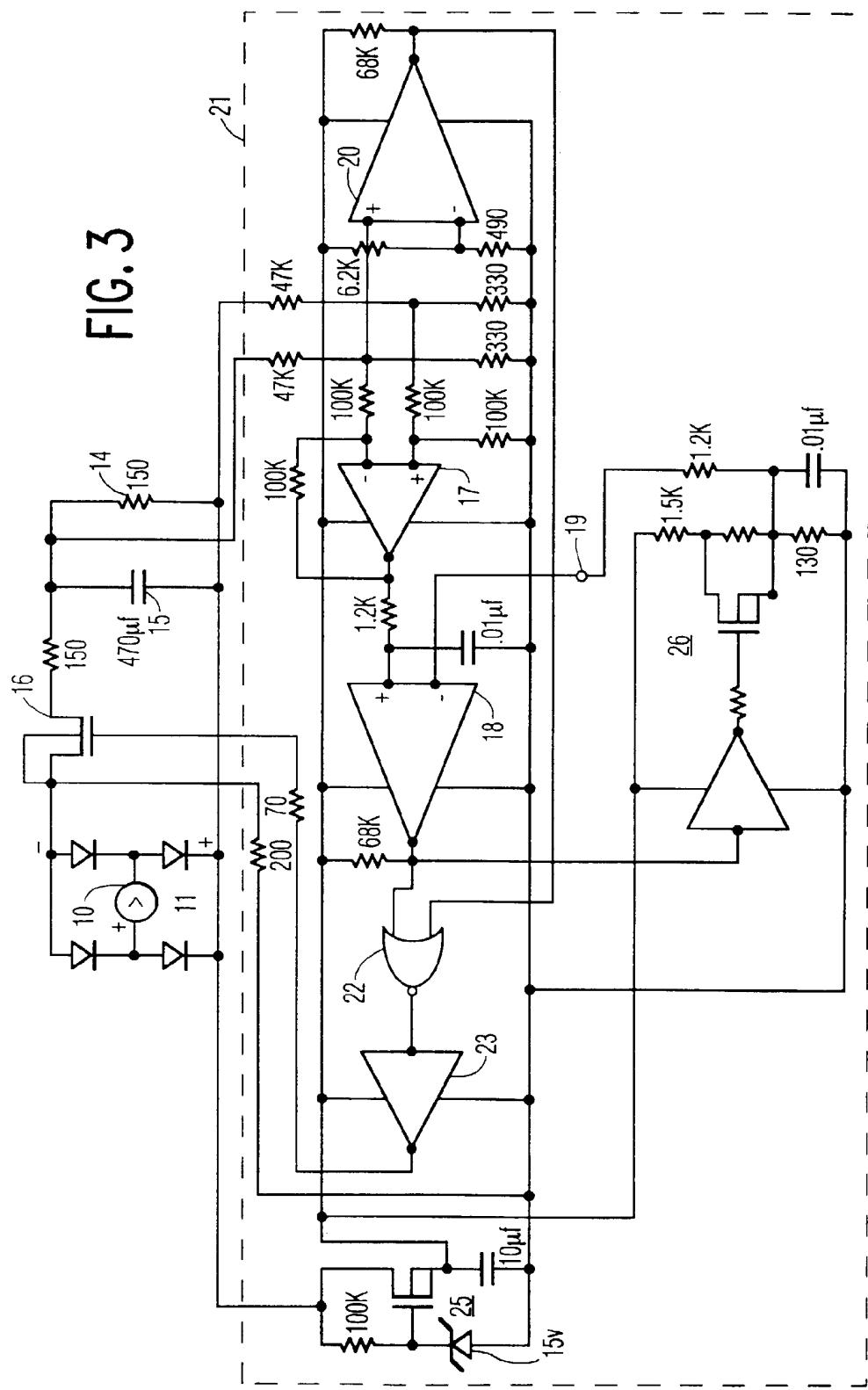


FIG. 2

FIG. 3





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## EUROPEAN PATENT APPLICATION

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⑯ Low power pre-regulator power supply circuit.

⑯ A power supply system employs a control circuit (21) to regulate the voltage across a load capacitor (15) by monitoring the capacitor voltage by means of a differential voltage sensor (17) and by monitoring the drain-source voltage of a switching power FET (16) connected in series with the load capacitor (15) across input terminals (12, 13) that supply a full wave rectified voltage derived from a commercial AC

supply voltage (10). The control circuit (21) controls the switching action of the power FET (16) in a manner such that the load capacitor (15) is charged at least once during each cycle of the rectified voltage (unfiltered). This method of voltage regulation by monitoring the load capacitor voltage and the FET voltage ( $V_{DS}$ ) provides significant advantages over other forms of voltage regulation.

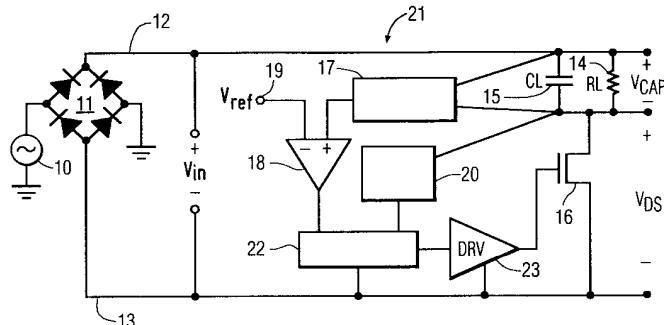


FIG. 1

BACKGROUND OF THE INVENTION

This invention relates to power supply circuits, and more particularly, to a low power transformerless, inductorless power supply circuit of the switching type.

One common form of power supply, which can be found in certain TV receivers, consists of a full wave bridge rectifier, a load capacitor (e.g. 330 $\mu$ F), and a linear regulator. The bridge rectifier generates a voltage which is filtered by the load capacitor. The load capacitor voltage is then fed to the linear regulator which in turn regulates the voltage at a preselected level, for example, 130V.

This power supply has certain disadvantages and limitations. For a 120V AC input, 170V is generated across the load capacitor of the bridge rectifier. Since the linear regulator must produce an output voltage of 130V, there is a 40V drop across the regulator itself, drawing up to 1 amp of current. In order to protect the regulator from damage due to the excessive amount of dissipated power, a number of thermal resistors are connected in parallel with the regulator so as to shunt a part of the current. These resistors are bulky and thus are undesirable as they increase the cost of the overall system and furthermore occupy a significant amount of space on the TV board. In addition, they allow only a small variation in the line voltage because if the voltage rating of the load capacitor is exceeded, damage to the load capacitor as well as the linear regulator may occur. This power supply therefore requires a well regulated 120V commercial line voltage. Since the load capacitor is charged only once for each half cycle of the AC supply voltage, higher peak capacitor charge currents result, along with other attendant difficulties.

U.S. Patent 4,685,046 (8/4/87) describes a transformerless, low voltage, direct current power supply of the switching type adapted to energize a low voltage direct current load. A full-wave bridge rectifier is coupled directly across a 115V, 60Hz alternating current line to provide a 120Hz pulsating direct current. A pair of transistors, alternately switching on and off in complementary fashion, continuously applies to a low power load only a leading edge portion and a trailing edge portion of each of the 120Hz direct current pulses. The resultant direct current voltage, e.g. 11.3 peak volts across the load, is thus substantially reduced to a desirable level as compared to the peak voltage (161 peak volts) of the pulsating direct current provided at the bridge output. In another embodiment, the function of the transistors is provided by a pair of operational amplifiers which control the switching of a field effect transistor in series with the load. The control function is provided by sensing the input voltage of the power supply circuit.

5 This has the disadvantage that if the input changes too abruptly and the sensor is not able to respond immediately to the change, the exact value of the output voltage cannot be well controlled. Furthermore, because the circuit threshold level is set by means of a zener diode, this makes the circuit less flexible in the event that the threshold has to be adjusted.

10 Another transformerless power supply which also senses the input supply voltage to determine the output voltage is described in DE 3304759- (8/16/84). In this German patent, a first op-amp compares a first input voltage, supplied by a full wave bridge rectifier, with a DC reference voltage supplied by a zener diode and a resistor voltage divider and a second op-amp compares a second input voltage with the DC reference voltage. If either input voltage is lower than the reference voltage, a switching transistor in series with a load capacitor is turned on. The load capacitor is only charged when the rectified AC supply voltage is below the reference voltage. The control function is once again provided by sensing the input voltage. This circuit uses a high-side power switch which produces higher power losses when compared with a low-side switch and results in problems in the integration thereof.

SUMMARY OF THE INVENTION

30 An object of the present invention is to provide an integrated circuit low cost power supply that produces a regulated DC voltage across a load capacitor from a wide input voltage range, in particular, one which can be used with both 120V and 220V AC line voltages.

35 Another object of the invention is to provide a power supply pre-regulator circuit that overcomes the disadvantages and limitations of known circuits of this type. In particular, one that senses the output voltage instead of the input voltage.

40 A further object of the invention is to provide a power supply pre-regulator circuit with reduced charging currents of the load capacitor while keeping the power dissipation to a minimum.

45 A still further object of the invention is to provide a power supply in which the switching losses in the switching transistor are kept low by monitoring the power switching transistor so that it is switched only when its drain-source voltage ( $V_{ds}$ ) is below a safe level, for example, 60V.

50 Another object of the invention is to provide a power supply system which eliminates the need for bulky thermal shunt resistors and hence reduces the thermal dissipation of the system.

55 These and other objects and advantages are achieved by means of a novel integrated circuit power supply system that charges a load capacitor

5 during the rising edge of the input cycle. The system includes a control circuit that senses the output voltage across the load capacitor and whenever the capacitor voltage exceeds a preset voltage level, for example, 150V, it turns off a series connected switching transistor, such as a field effect transistor (FET), which stops the load capacitor from being charged. The full-wave rectified AC sinusoidal supply voltage is applied to the series circuit of the load capacitor and the switching transistor and, during the falling edge of the rectified half cycle of the supply voltage, the control circuit senses when the drain-source voltage of the switching transistor reaches a preset safe level (e.g. 60V) and in response switches on the power switching transistor to charge the load capacitor for a second time during that cycle until the input voltage drops below the capacitor voltage. The transistor switch remains on so that on the next leading (rising) edge of the rectified supply voltage, i.e. when the supply voltage again exceeds the load capacitor voltage, the load capacitor is once again recharged. The control circuit then switches off the series connected switching transistor when the load capacitor voltage (i.e., the output voltage) again exceeds the preset voltage level (e.g. 150V). In this way, the load capacitor is charged twice during each half cycle of the AC supply voltage (or twice during each cycle of the rectified pulsatory voltage at the output of the full wave bridge rectifier circuit).

10 The load voltage can thus be regulated to any preset threshold level that is determined by a reference voltage. Unlike previous methods, this level would not be affected by the amplitude or rate of change of the input voltage. The switching transistor is a low-side switch in common source configuration which has the advantages of low power loss and ease of implementation and integration. The dual charging technique of the load capacitor minimizes the ripple voltage across the load.

15 An advantage of this so-called output sensing approach in which the load capacitor voltage and the switching transistor drain-source voltage are monitored rather than the input voltage is that it maintains direct control of the load capacitor voltage while charging the capacitor twice in each cycle. This has a very real advantage in that the output voltage can be more accurately regulated over a much wider range of input voltage.

20 To summarize, the control circuit senses the load capacitor voltage and when it exceeds the preset level (e.g. 150V), the switching transistor is turned off. The control circuit also senses the drain-source voltage and allows the switching transistor to be turned back on when its drain-source voltage falls below a safe level (e.g. 60V). This allows the load capacitor to be charged a second time to

25 produce a second peak. The switching losses are kept to a minimum by switching the switching transistor only when its drain-source voltage is below the safe level. The peak charging currents of the load capacitor are maintained at a low value and the circuit power dissipation is kept at a minimum.

#### BRIEF DESCRIPTION OF THE DRAWINGS

10

A fuller understanding of the invention together with other features, objects and advantages thereof will become apparent from the following detailed description taken in conjunction with the accompanying drawings, in which:

15 Fig. 1 illustrates a simplified block diagram of a preferred embodiment of a power supply in accordance with the present invention,

20 Fig. 2 provides waveform diagrams illustrating the operation of the circuit of Fig. 1, and

25 Fig. 3 is a more complete schematic circuit diagram showing one way in which the invention shown in Fig. 1 can be realized.

#### DESCRIPTION OF THE PREFERRED EMBODIMENTS

30 Fig. 1 shows a block diagram of a pre-regulator power supply employing the capacitor dual charging concept of the present invention. A conventional, commercial power source 10 of 115V or 220V sinusoidal alternating current at a frequency of 60Hz or the like is coupled to a pair of input terminals of a full-wave bridge rectifier 11 made up of four diodes. The output of the bridge will provide a pulsating rectified voltage,  $V_{in}$ , between a positive voltage line 12 and a negative voltage line 13.

35 An electric load 14 is connected in parallel with a filter or load capacitor 15 and this parallel combination is connected in series circuit with a switching transistor 16 of a power FET type that can handle the load current. The switching transistor 16 is preferably connected to the low voltage side of the DC supply voltage which thus simplifies its integration into an integrated circuit. The field effect transistor is preferably chosen to be an LIGBT power device or an LDMOS device. Of course, the invention is not limited to this choice of the power devices.

40 45 50 55 50 A control circuit 21 includes a subtractor circuit 17 which is coupled across the terminals of the load capacitor 15 in order to sense the capacitor voltage. A means for differential voltage sensing is required rather than a single-ended voltage sensor. The subtractor circuit 17 may or may not include a hysteresis circuit, which helps suppress any spurious inputs caused by ringing produced during turnoff of the switching transistor 16.

The output of the subtractor circuit 17 is connected to the non-inverting input (+) of a comparator 18. The inverting input (-) of the comparator 18 is connected to a terminal 19 which supplies a preset reference voltage,  $V_{ref}$ . The reference voltage  $V_{ref}$  determines the voltage level at which the comparator 18 will change state and can be adjustable, if desired. In one example, useful in a TV receiver, the reference voltage  $V_{ref}$  was selected so that the comparator 18 changes state when the load capacitor voltage  $V_{cap}$  across the load capacitor 15 exceeds 150V.

A sensor circuit 20 is provided in order to sense the drain-source voltage  $V_{ds}$  of the switching transistor 16. As will be shown below, the  $V_{ds}$  sensor circuit 20 may comprise a second comparator circuit which compares the voltage  $V_{ds}$  of the switching transistor 16 to a reference voltage which, in the present example, is chosen so that the second comparator will change state when the drain-source voltage of the power switching transistor drops below 60V.

An output of the comparator circuit 18 and of the  $V_{ds}$  sensor circuit 20 are each connected to a respective input of a logic circuit 22, which in its simplest form could consist of a NOR gate.

The output of the logic circuit 22 is in turn coupled to an input of a driver amplifier 23. The output of the driver amplifier is coupled to the gate electrode of the power switching transistor 16.

A pair of DC output terminals coupled to the load capacitor 15 can supply the load capacitor voltage to a linear regulator circuit or the like (not shown).

The operation of the circuit of Fig. 1 will be described in connection with the voltage waveform diagram shown in Fig. 2. The bridge rectifier 11 circuit supplies a rectified pulsating voltage waveform  $V_{in}$  as shown in Fig. 2. In the case of a 60Hz AC supply voltage, the voltage  $V_{in}$  has frequency of 120Hz. The voltage  $V_{in}$  is applied across the series circuit consisting of the load capacitor 15 and the switching transistor 16.

The function of the control circuit 21 is to regulate the voltage  $V_{cap}$  across the load capacitor 15 to a preset voltage level, for example, 150V DC, despite the fact that the input voltage  $V_{in}$  has a peak value that is higher than the preset voltage. Initially, assuming the load capacitor 15 is uncharged, the switching transistor 16 is turned on fully so that substantially the entire voltage  $V_{in}$  is across the load capacitor 15. This will allow the load capacitor 15 to be charged as the voltage  $V_{in}$  rises, i.e. as  $V_{in}$  rises in voltage, the capacitor voltage  $V_{cap}$  also increases.

The subtractor circuit 17 continuously monitors the differential voltage  $V_{cap}$  and by means of the comparator 18 compares  $V_{cap}$  with a preset refer-

ence voltage,  $V_{ref}$ , supplied to the inverting input of the comparator 18. When the load capacitor voltage  $V_{cap}$  reaches the preset level, i.e. 150V in the example chosen, the comparator circuit 18 changes state.

The logic circuit 22 responds to the output signal of the comparator circuit 18 to drive the switching transistor 16 into cut-off via a gate turn-off voltage applied to the gate of the switching transistor 16 via the driver amplifier 23. This prevents further charging of the load capacitor 15 as the input voltage  $V_{in}$  increases further in value above the 150V level. This produces a first peak in the capacitor voltage waveform at the instant labelled  $t_1$  on the waveform of Fig. 2. The waveform diagram of Fig. 2 also shows the switch gate voltage waveform  $V_{sw}$ , which goes low at the instant  $t_1$  when the switching transistor is turned off. During the time period after the switch turns off at  $t_1$ , the capacitor discharges slowly through the load resistor 14, as shown by the capacitor waveform  $V_{cap}$  in Fig. 2.

As the voltage  $V_{in}$  continues to increase and the load capacitor 15 continues to discharge, the subtractor circuit 17 may include a hysteresis circuit to maintain the comparator circuit 18 in the state to hold the switching transistor 16 off via the logic and driver stages 22 and 23. The hysteresis circuit can be implemented by changing the value of the reference voltage  $V_{ref}$  when the comparator 18 switches states. During the time period when the switching transistor 16 is turned off, the drain-source voltage of switching transistor 16 can exceed 60V.

After the voltage  $V_{in}$  reaches its peak value and begins its descent, the drain-source voltage,  $V_{ds}$ , of the switching transistor 16 will begin to decrease. The voltage  $V_{ds}$  satisfies the relation,

$$V_{ds} = V_{in} - V_{cap}.$$

When the voltage  $V_{ds}$  drops below a second preset level, in the present example, 60V, the  $V_{ds}$  sensor circuit 20 will be triggered to change state and in turn cause the logic circuit 22 to turn the switching transistor 16 back on. This will occur at the instant  $t_2$  in the waveform diagram of Fig. 2 and produces a second peak in the load capacitor voltage waveform  $V_{cap}$  as the load capacitor recharges towards the voltage  $V_{in}$ . The waveform diagram of Fig. 2 also shows the switch voltage waveform  $V_{sw}$  going high at  $t_2$  when the switching transistor 16 is turned on. It is also possible to set the  $V_{ds}$  sensor circuit to a threshold level of zero volts, in which case the circuit will not produce the second voltage peak at time  $t_2$ .

As the voltage,  $V_{in}$ , continues its descent and drops below the capacitor voltage  $V_{cap}$  in the period between  $t_2$  and  $t_3$ , the switching transistor 16

will stay on (be conductive), but will not continue to charge the load capacitor 15 when the voltage  $V_{in}$  has dropped below the value of the capacitor voltage  $V_{cap}$ .

On the rising edge of the next cycle, the voltage,  $V_{in}$ , will increase again until at the instant  $t_3$  when  $V_{in}$  exceeds the capacitor voltage  $V_{cap}$ , the load capacitor 15 will begin to charge again through the still conductive switching transistor 16. The first peak in the capacitor voltage  $V_{cap}$  waveform at a value of 150V will then reappear as the cycle described now repeats itself. The switching transistor 16 will again be turned off when the subtractor circuit senses a differential voltage of 150V across the load capacitor 15.

It can thus be seen that the control circuit 21 allows the load capacitor 15 to be charged twice during each cycle of the rectified voltage waveform  $V_{in}$  (i.e. twice during each half cycle of the AC supply voltage 10). The subtractor circuit 17 initiates the first peak in the capacitor voltage waveform  $V_{cap}$  and the  $V_{ds}$  sensor initiates circuit 20 the second peak. This technique allows the load capacitor 15 to be charged twice in each half cycle of the AC supply voltage thereby lowering the peak charging current flowing to the load capacitor as compared to known methods in which the capacitor is charged only once for each half cycle of the AC supply voltage. The lower peak charging currents resulting from the invention produce lower stresses on the switching transistor 16 and the lower value of  $V_{ds}$  during switching of the switching transistor reduces the switching losses and also the power dissipation. This increases the circuit efficiency and also makes it possible to use a switching transistor that is less expensive since it will be subjected to lower voltages during switching etc.

As can be seen from the foregoing description, the invention can extend the input voltage range of a TV receiver or other electronic apparatus from 120V to 220V or more by limiting the voltage across the load capacitor to a preset level, such as 150V, even if the input voltage reaches a value of 265V, AC (375V peak). The system described insures that the load capacitor voltage does not exceed 150V irrespective of the value of the line voltage. Switching losses are minimal as the switching transistor always switches when the input voltage is about 150V and the drain-source voltage is low. The load capacitor voltage is very well controlled since the capacitor voltage is itself used as the control parameter.

Fig. 3 shows one possible way to realize the complete system of Fig. 1 with the control circuit 21 indicated by dashed lines. Elements which are the same as those in Fig. 1 have the same reference labels. The subtractor formed by the op-amp 17 attenuates and differentially senses the load

capacitor voltage. The subtractor output voltage is then compared to a reference voltage using the comparator 18. The reference voltage has been selected so that the comparator changes state when the load capacitor voltage exceeds 150V. The second comparator 20 is used to sense the drain-source voltage of the FET 16. The Input terminals of the second comparator 20 are coupled, either directly or via some means of attenuation, to the drain electrode and the source electrode of the field effect transistor 16. Additional logic 22 uses the signals from the two comparators 18 and 20 to control the turn on and turn off of the power FET 16.

In addition to the functional blocks shown in Fig. 1, the control circuit of Fig. 3 also includes a low voltage supply circuit 25 which provides a regulated low DC voltage for energizing the low voltage circuits of the control circuit 21. Fig. 3 also provides a hysteresis circuit 26 which changes the level of the reference voltage supplied to the inverting input of comparator 18 via the reference voltage terminal 19. The duration of the subtractor signal voltage is thereby lengthened by the operation of the hysteresis circuit. The hysteresis circuit is itself conventional. The system of Fig. 3 operates in accordance with the description of the operation of the circuit of Fig. 1 and thus requires no further elaboration.

Although a preferred embodiment of the invention has been shown and described, it should be understood that various modifications, deletions and rearrangements of the parts may be resorted to without departing from the spirit and scope of the invention as disclosed and claimed herein.

## Claims

1. A switching type regulated power supply for energizing a load comprising:  
40 first and second input terminals for supplying a pulsatory type rectified voltage to the power supply,  
45 means for coupling a load capacitor and a switching transistor in a series circuit across the first and second input terminals so that the switching transistor controls current flow through the load capacitor,  
50 a pair of output terminals coupled to the load capacitor, and  
55 a control circuit having input means coupled to the load capacitor and to the switching transistor and an output coupled to a control electrode of the switching transistor, said control circuit including means responsive to a differential voltage of the load capacitor and a voltage produced across the switching transistor for controlling the switching transistor in a

manner so as to charge the load capacitor twice during each cycle of the pulsatory rectified voltage.

2. A switching type regulated power supply as claimed in Claim 1 wherein the control circuit comprises;

a first network coupled to the load capacitor and responsive to the load capacitor differential voltage for deriving a first switch-type control signal for driving the switching transistor into cut-off at a given voltage level of the load capacitor voltage, and

a second network coupled to the switching transistor and responsive to the transistor voltage for deriving a second switch-type control signal for driving the switching transistor into conduction at a given voltage of the switching transistor.

3. A switching type regulated power supply as claimed in Claim 2 wherein the control circuit further comprises;

a logic means controlled by said first and second switch-type control signals for supplying a trigger control signal to a control electrode of the switching transistor.

4. A switching type regulated power supply as claimed in Claim 1, 2 or 3 wherein said first and second input terminals comprise a high side voltage and a low side voltage, respectively, and said load capacitor and said switching transistor are connected between the first and second input terminals in the order named.

5. A switching type regulated power supply as claimed in Claim 2, 3 or 4 wherein;

said first network comprises a subtractor circuit having its input coupled to the load capacitor and having its output coupled to a first input of a comparator, and wherein a second input of the comparator is coupled to a reference voltage that determines said given cut-off voltage level.

6. A switching type regulated power supply as claimed in Claim 2, 3 4 or 5 wherein the second network comprises a second comparator having its input coupled across the switching transistor.

7. A switching type regulated power supply as claimed in Claim 6 wherein the switching transistor comprises a field effect transistor having a drain electrode and a source electrode and the input of the second comparator includes

first and second terminals coupled to the drain electrode and the source electrode, respectively, of the field effect transistor.

5 8. A switching type regulated power supply as claimed in Claim 1, 2, 3, 4, 5, 6 or 7 further comprising a full wave bridge rectifier having first and second output terminals coupled to said first and second input terminals, respectively, and a pair of input terminals coupling to a source of sinusoidal AC voltage.

10 9. A switching type regulated power supply as claimed in Claim 8 wherein said bridge rectifier supplies a rectified sine wave voltage to said first and second input terminals and said control circuit is operative to turn off the switching transistor at a given voltage level on the leading edge of the rectified sine wave voltage and to turn on the switching transistor during the trailing edge of the sine wave voltage and at a preset voltage developed across the switching transistor.

15 20 25 10. A switching type regulated power supply as claimed in Claim 1, 2, 3, 4, 5, 6, 7, 8 or 9 wherein the control circuit turns off the switching transistor at a first predetermined voltage level of the output load capacitor voltage which is less than the peak input voltage value of the pulsatory type rectified voltage and turns on the switching transistor at a second predetermined voltage level of the switching transistor.

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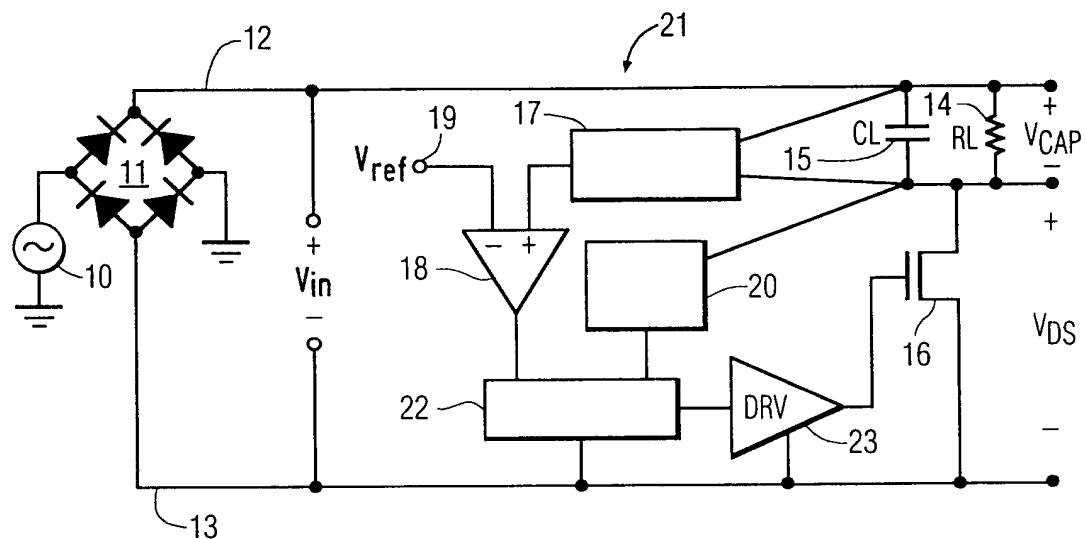


FIG. 1

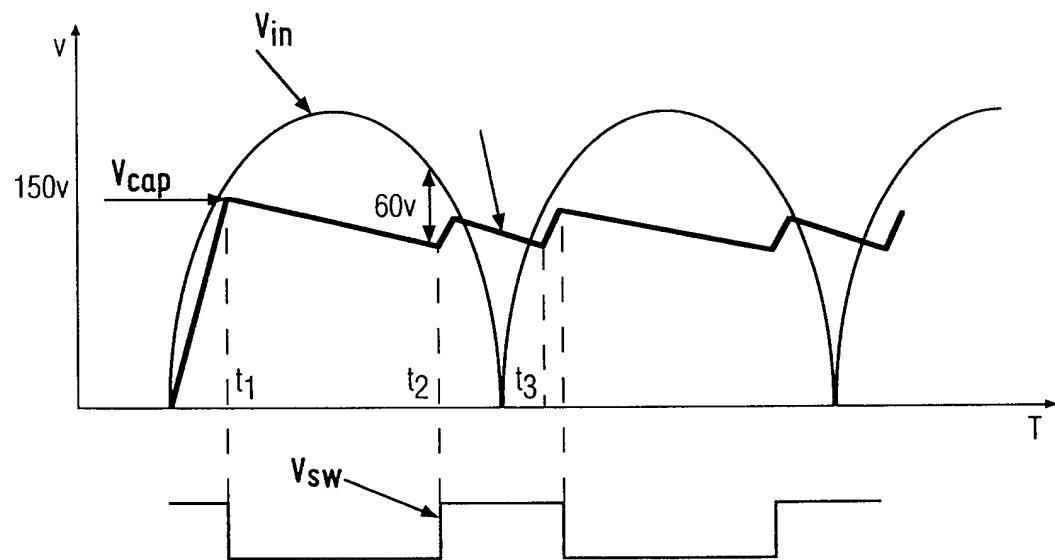
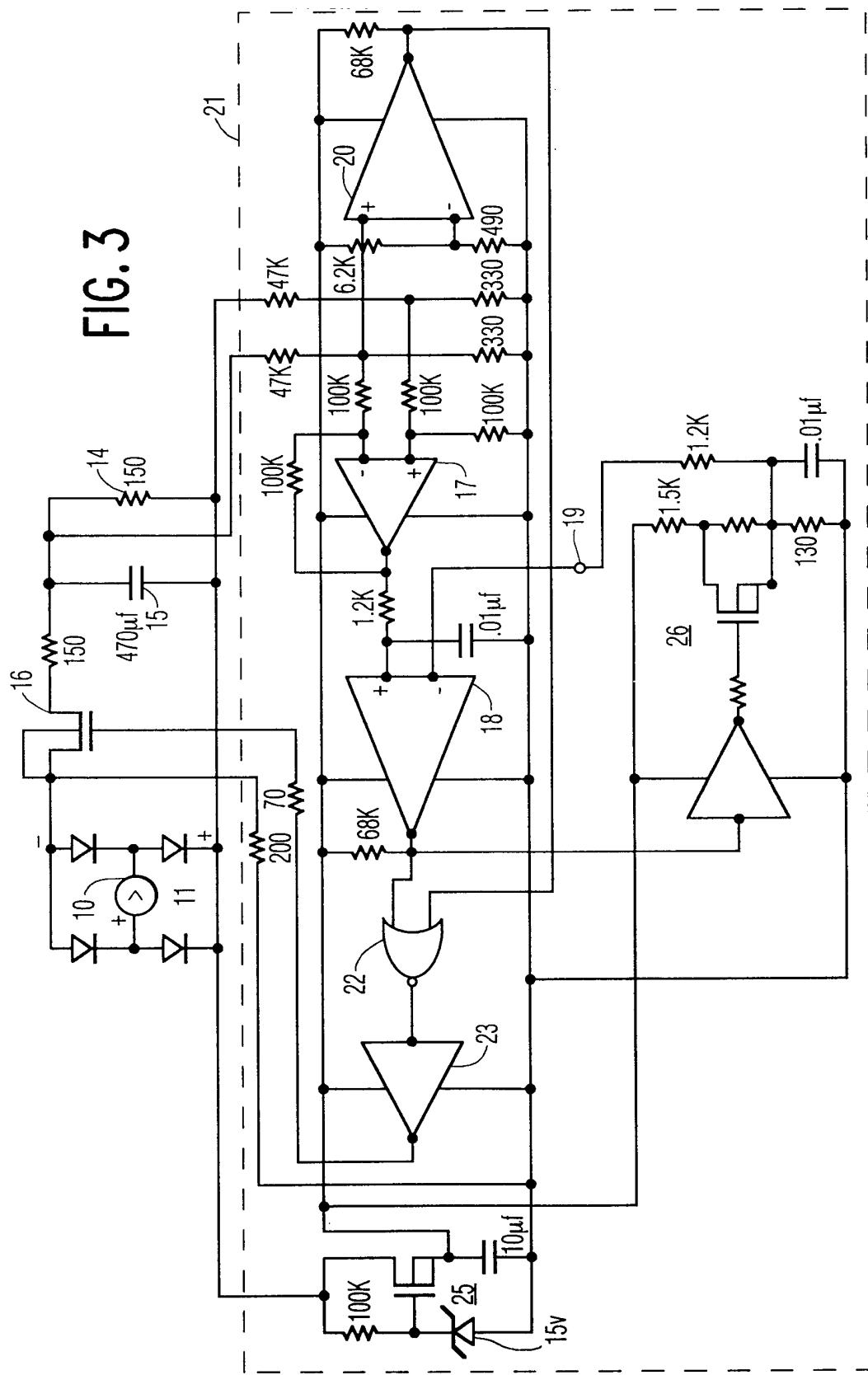


FIG. 2

FIG. 3





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## EUROPEAN PATENT APPLICATION

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⑮ Int. Cl. 5: **H02M 3/156, H02M 7/217**

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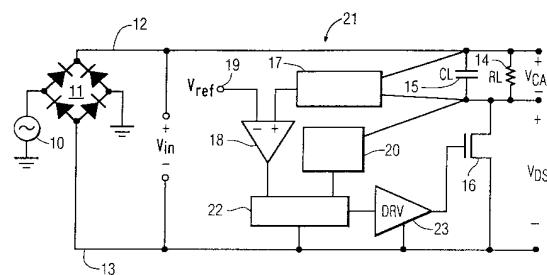
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㉕ **Low power pre-regulator power supply circuit.**

㉖ A power supply system employs a control circuit (21) to regulate the voltage across a load capacitor (15) by monitoring the capacitor voltage by means of a differential voltage sensor (17) and by monitoring the drain-source voltage of a switching power FET (16) connected in series with the load capacitor (15) across input terminals (12, 13) that supply a full wave rectified voltage derived from a commercial AC supply voltage (10). The control circuit (21) controls the switching action of the power FET (16) in a manner such that the load capacitor (15) is charged at least once during each cycle of the rectified voltage (unfiltered). This method of voltage regulation by monitoring the load capacitor voltage and the FET voltage ( $V_{ds}$ ) provides significant advantages over other forms of voltage regulation.



**FIG. 1**



European Patent  
Office

## EUROPEAN SEARCH REPORT

Application Number  
EP 94 20 1128

DOCUMENTS CONSIDERED TO BE RELEVANT			
Category	Citation of document with indication, where appropriate, of relevant passages	Relevant to claim	CLASSIFICATION OF THE APPLICATION (Int.Cl.5)
Y	EP-A-0 256 569 (PHILIPS) * the whole document * ---	1, 4, 5, 8	H02M3/156 H02M7/217
D, Y	DE-A-33 04 759 (SIEMENS) * the whole document * ---	1, 4, 5, 8	
A	GB-A-2 208 019 (DIEHL) * page 2, column 11 - page 3, column 30; figures 1-5 * -----	1-10	
TECHNICAL FIELDS SEARCHED (Int.Cl.5)			
H02M			
The present search report has been drawn up for all claims			
Place of search THE HAGUE	Date of completion of the search 4 November 1994	Examiner Gentili, L	
CATEGORY OF CITED DOCUMENTS	<p>T : theory or principle underlying the invention E : earlier patent document, but published on, or after the filing date D : document cited in the application L : document cited for other reasons ..... &amp; : member of the same patent family, corresponding document</p>		
X : particularly relevant if taken alone Y : particularly relevant if combined with another document of the same category A : technological background O : non-written disclosure P : intermediate document			